Picoamp Input Current, Microvolt Offset, Low Noise Op Amp

FEATURES

- *Guaranteed* Bias Current
  - 25°C .... 100pA max.
  - −55°C to 125°C .... 600pA max.
- *Guaranteed* Offset Voltage .... 120μV max.
- *Guaranteed* Drift .... 1.5μV/°C max.
- Low Noise, 0.1Hz to 10Hz 0.5μVp-p
- *Guaranteed* Low Supply Current .... 600μA max.
- *Guaranteed* CMRR .... 114 dB min.
- *Guaranteed* PSRR .... 114 db min.
- *Guaranteed* Voltage Gain with 5mA load current

APPLICATIONS

- Precision instrumentation
- Charge integrators
- Wide dynamic range logarithmic amplifiers
- Light meters
- Low frequency active filters
- Standard cell buffers
- Thermocouple amplifiers

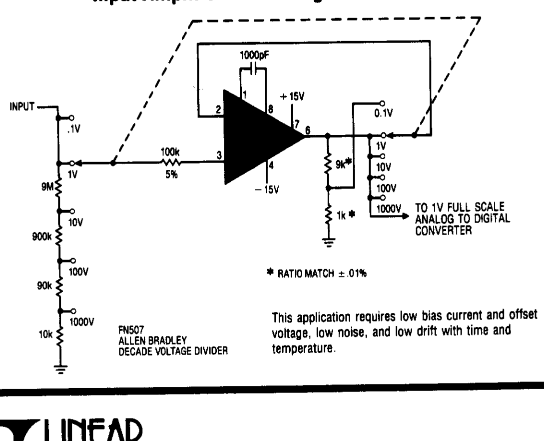
DESCRIPTION

The LT1008 is a universal precision operational amplifier which can be used in practically all precision applications. The LT1008 combines for the first time picoampere bias currents (which are maintained over the full −55°C to 125°C temperature range) microvolt offset voltage (and low drift with time and temperature), low voltage and current noise, and low power dissipation. Extremely high common-mode and power supply rejection ratios, and the ability to deliver 5mA load current with high voltage gain round out the LT1008's superb precision specifications.

The all around excellence of the LT1008 eliminates the necessity of the time consuming error analysis procedure of precision system design in many applications; the LT1008 can be stocked as the universal precision op amp.

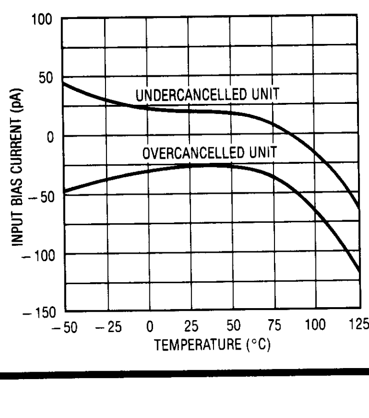
The LT1008 is externally compensated with a single capacitor for additional flexibility in shaping the frequency response of the amplifier. It plugs into and upgrades all standard LM108A/308A applications. For an internally compensated version with even lower offset voltage but otherwise similar performance see the LT1012.

Input Amplifier for 4½ Digit Voltmeter



This application requires low bias current and offset voltage, low noise, and low drift with time and temperature.

Input Bias Current vs Temperature

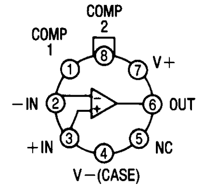


ABSOLUTE MAXIMUM RATING

Supply Voltage........................ ±20V
Differential Input Current (Note 1)......... ±10mA
Input Voltage .... ±20V
Output Short Circuit Duration........... Indefinite
Operating Temperature Range
  LT1008M .... −55°C to 125°C
  LT1008C .... 0°C to 70°C
Storage Temperature Range
  All Devices................. −65°C to 150°C
Lead Temperature (Soldering, 10 sec.)...... 300°C

PACKAGE/ORDER INFORMATION

TOP VIEW

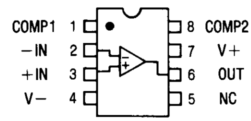


METAL CAN H PACKAGE

ORDER PART NO.

LT1008MH
LT1008CH

TOP VIEW



PLASTIC DIP N8 PACKAGE

LT1008CN8

ELECTRICAL CHARACTERISTICS $V_S = \pm15V$, $V_{CM} = 0V$, $T_A = 25°C$, unless otherwise noted.

SYMBOL	PARAMETER	CONDITIONS	LT1008M MIN	LT1008M TYP	LT1008M MAX	LT1008C MIN	LT1008C TYP	LT1008C MAX	UNITS
V_{OS}	Input Offset Voltage			30	120		30	120	μV
		Note 2		40	180		40	180	μV
	Long Term Input Offset Voltage Stability			0.3			0.3		μV/month
I_{OS}	Input Offset Current			30	100		30	100	pA
		Note 2		40	150		40	150	pA
I_B	Input Bias Current			±30	±100		±30	±100	pA
		Note 2		±40	±150		±40	±150	pA
e_n	Input Noise Voltage	0.1Hz to 10Hz		0.5			0.5		μVp-p
e_n	Input Noise Voltage Density	f_0 = 10Hz (Note 3)		17	30		17	30	$nV/\sqrt{Hz}$
		f_0 = 1000Hz (Note 4)		14	22		14	22	$nV/\sqrt{Hz}$
i_n	Input Noise Current Density	f_0 = 10Hz		20			20		$fA/\sqrt{Hz}$
A_{VOL}	Large Signal Voltage Gain	$V_{OUT} = \pm12V$, $R_L \geq 10k\Omega$	200	2000		200	2000		V/mV
		$V_{OUT} = \pm10V$, $R_L \geq 2k\Omega$	120	600		120	600		V/mV
CMRR	Common Mode Rejection Ratio	$V_{CM} = \pm13.5V$	114	132		114	132		dB
PSRR	Power Supply Rejection Ratio	$V_S = \pm2V$ to $\pm20V$	114	132		114	132		dB
	Input Voltage Range		±13.5	±14.0		±13.5	±14.0		V
V_{OUT}	Output Voltage Swing	$R_L = 10k\Omega$	±13	±14		±13	±14		V
	Slew Rate	$C_f = 30pF$	0.1	0.2		0.1	0.2		V/μsec
I_S	Supply Current	Note 2		380	600		380	600	μA

LINEAR TECHNOLOGY

ELECTRICAL CHARACTERISTICS $V_S = \pm15V$, $V_{CM} = 0V$, $0°C \leq T_A \leq 70°C$ for the LT1008C and $-55°C \leq T_A \leq 125°C$ for the LT1008M, unless otherwise noted.

SYMBOL	PARAMETER	CONDITIONS		LT1008M MIN	LT1008M TYP	LT1008M MAX	LT1008C MIN	LT1008C TYP	LT1008C MAX	UNITS
V_{OS}	Input Offset Voltage		●		50	250		40	180	μV
		Note 2	●		60	320		50	250	μV
	Average Temperature Coefficient of Input Offset Voltage		●		0.2	1.5		0.2	1.5	μV/°C
I_{OS}	Input Offset Current		●		60	250		40	180	pA
		Note 2	●		80	350		50	250	pA
	Average Temperature Coefficient of Input Offset Current		●		0.4	2.5		0.4	2.5	pA/°C
I_B	Input Bias Current		●		±80	±600		±40	±180	pA
		Note 2	●		±150	±800		±50	±250	pA
	Average Temperature Coefficient of Input Bias Current		●		0.6	6.0		0.4	2.5	pA/°C
A_{VOL}	Large Signal Voltage Gain	$V_{OUT} = \pm12V$, $R_L \geq 10k\Omega$	●	100	1000		150	1500		V/mV
CMRR	Common Mode Rejection Ratio	$V_{CM} = \pm13.5V$	●	108	128		110	130		dB
PSRR	Power Supply Rejection Ratio	$V_S = \pm2.5V$ to $\pm20V$	●	108	126		110	128		dB
	Input Voltage Range		●	±13.5			±13.5			V
V_{OUT}	Output Voltage Swing	$R_L = 10k\Omega$	●	±13	±14		±13	±14		V
I_S	Supply Current		●		400	800		400	800	μA

The ● denotes the specifications which apply over the full operating temperature range.

Note 1: Differential input voltages greater than 1V will cause excessive current to flow through the input protection diodes unless current limiting resistors are used.

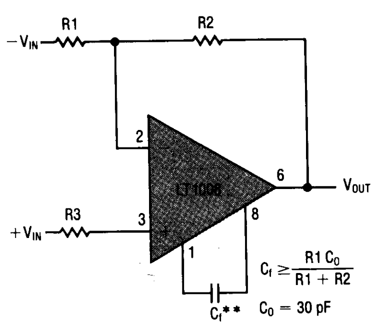
Note 2: These specifications apply for $\pm2V \leq V_S \leq \pm20V$ ($\pm2.5V \leq V_S \leq \pm20V$ over the temperature range) and $-13.5V \leq V_{CM} \leq 13.5V$ (for $V_S = \pm15V$).

Note 3: 10Hz noise voltage density is sample tested on every lot. Devices 100% tested at 10Hz are available on request.

Note 4: This parameter is tested on a sample basis only.

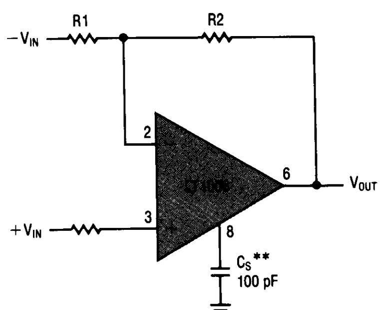
FREQUENCY COMPENSATION CIRCUITS

Standard Compensation Circuit



** BANDWIDTH AND SLEW RATE ARE PROPORTIONAL TO $1/C_f$

Alternate* Frequency Compensation



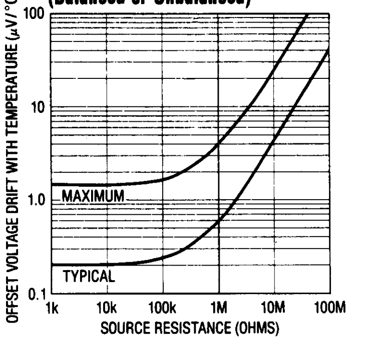
* IMPROVES REJECTION OF POWER SUPPLY NOISE BY A FACTOR OF 5.

** BANDWIDTH AND SLEW RATE ARE PROPORTIONAL TO $1/C_S$

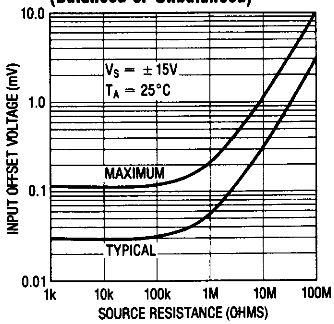
FOR $\frac{R2}{R1} > 200$ NO EXTERNAL FREQUENCY COMPENSATION IS NECESSARY

TYPICAL PERFORMANCE CHARACTERISTICS

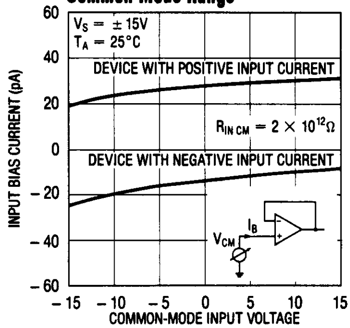
Offset Voltage Drift vs Source Resistance (Balanced or Unbalanced)



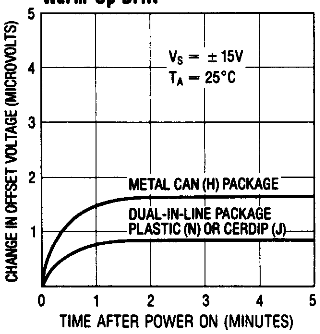
Offset Voltage vs Source Resistance (Balanced or Unbalanced)



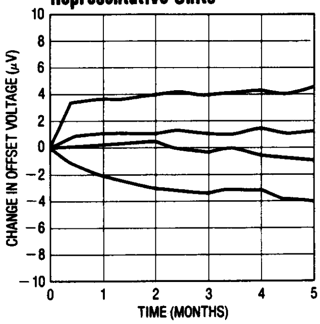
Input Bias Current Over Common Mode Range



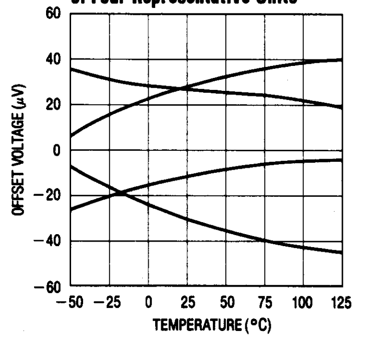
Warm-Up Drift



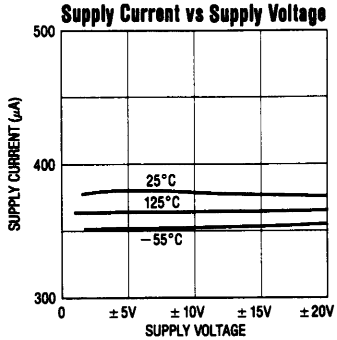
Long Term Stability of Four Representative Units



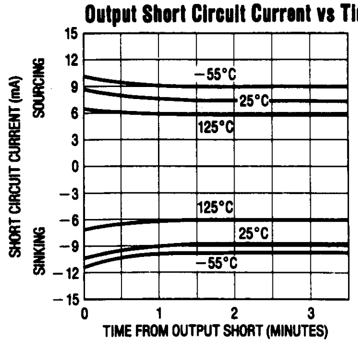
Offset Voltage Drift with Temperature of Four Representative Units



Supply Current vs Supply Voltage



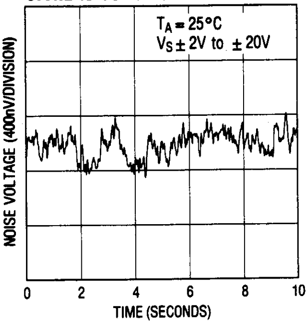
Output Short Circuit Current vs Time



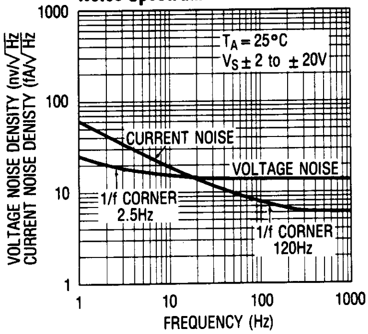
LINEAR TECHNOLOGY

TYPICAL PERFORMANCE CHARACTERISTICS

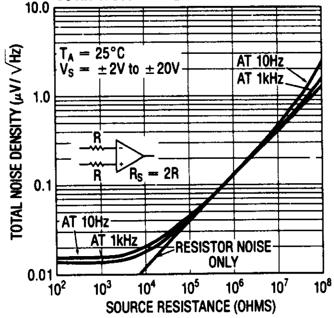
0.1Hz to 10Hz Noise



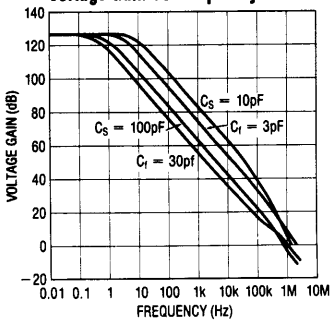
Noise Spectrum



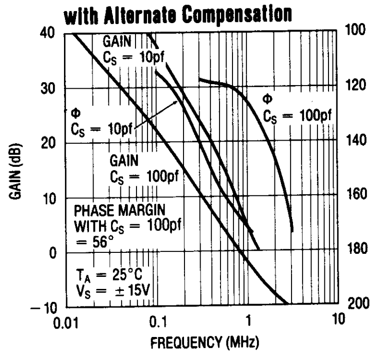
Total Noise vs Source Resistance



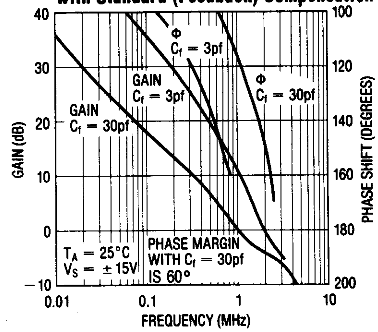
Voltage Gain vs Frequency



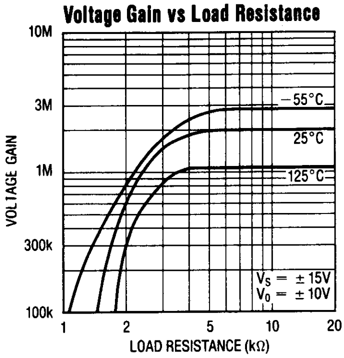
Gain, Phase Shift vs Frequency with Alternate Compensation



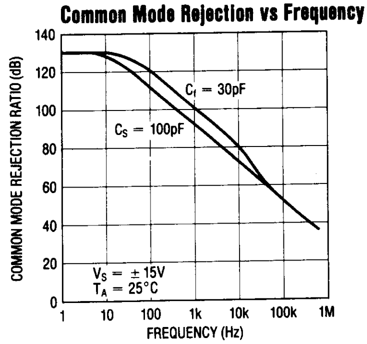
Gain, Phase Shift vs Frequency with Standard (Feedback) Compensation



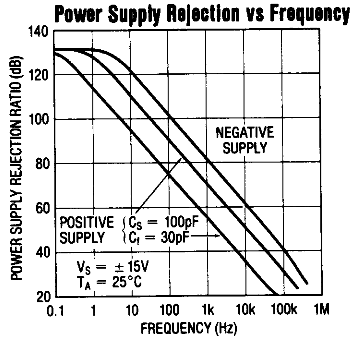
Voltage Gain vs Load Resistance



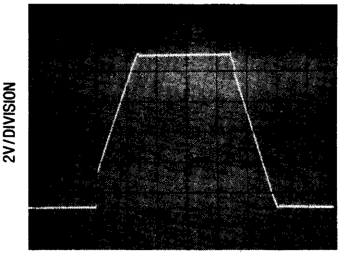
Common Mode Rejection vs Frequency



Power Supply Rejection vs Frequency

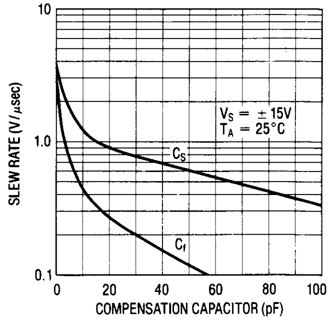


Large Signal Transient Response

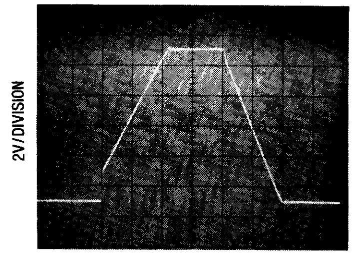


$A_V = +1$, $C_S = 100pF$, 20μsec/DIV

Slew Rate vs Compensation Capacitance

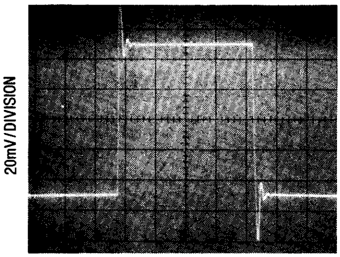


Large Signal Transient Response



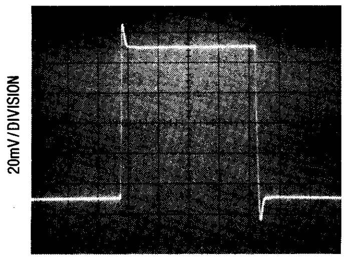
$A_V = +1$, $C_f = 30pF$, 20μsec/DIV

Small Signal Transient Response



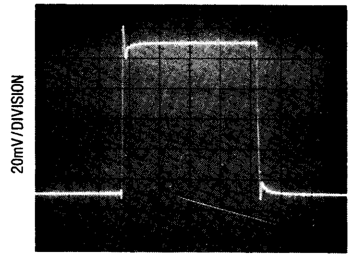
$A_V = +1$, $C_S = 100pF$, $C_{LOAD} = 100pF$, 5μsec/DIV

Small Signal Transient Response



$A_V = +1$, $C_S = 100pF$, $C_{LOAD} = 600pF$, 5μsec/DIV

Small Signal Transient Response



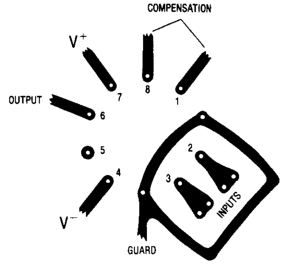
$A_V = +1$, $C_f = 30pF$, $C_{LOAD} = 100pF$, 5μsec/DIV

APPLICATIONS INFORMATION

Achieving Picoampere/Microvolt Performance

In order to realize the picoampere — microvolt level accuracy of the LT1008, proper care must be exercised. For example, leakage currents in circuitry external to the op amp can significantly degrade performance. High quality insulation should be used (e.g. Teflon, Kel-F); cleaning of all insulating surfaces to remove fluxes and other residues will probably be required. Surface coating may be necessary to provide a moisture barrier in high humidity environments.

Board leakage can be minimized by encircling the input circuitry with a guard ring operated at a potential close to that of the inputs: in inverting configurations the guard ring should be tied to ground, in non-inverting connections to the inverting input at pin 2. Guarding both sides of the printed circuit board is required. Bulk leakage reduction depends on the guard ring width. Nanoampere level leakage into the compensation terminals can affect offset voltage and drift with temperature.

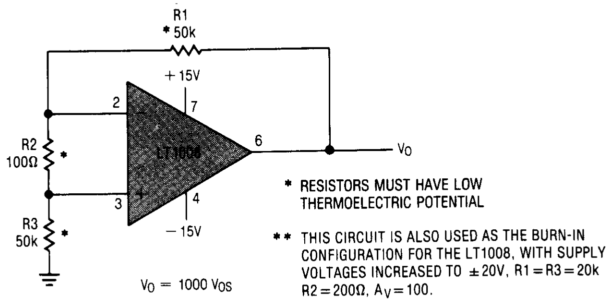


APPLICATIONS INFORMATION

Microvolt level error voltages can also be generated in the external circuitry. Thermocouple effects caused by temperature gradients across dissimilar metals at the contacts to the input terminals can exceed the inherent drift of the amplifier. Air currents over device leads should be minimized, package leads should be short, and the two input leads should be as close together as possible and maintained at the same temperature.

The LT1008 is specified over a wide range of power-supply voltages from ±2V to ±18V. Operation with lower supplies is possible down to ±1.0V (two Ni-Cad-batteries).

Test Circuit for Offset Voltage and its Drift with Temperature



Noise Testing

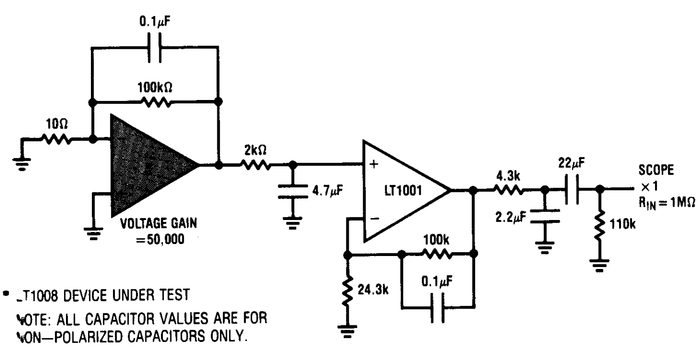
The 0.1Hz to 10Hz peak-to-peak noise of the LT1008 is measured in the test circuit shown. The frequency response of this noise tester indicates that the 0.1Hz corner is defined by only one zero. The test time to measure 0.1Hz to 10Hz noise should not exceed 10 seconds, as this time limit acts as an additional zero to eliminate noise contributions from the frequency band below 0.1Hz.

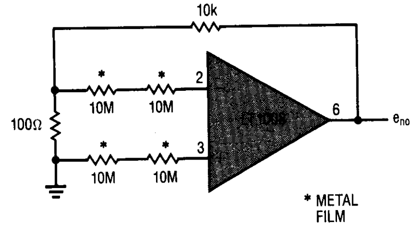
A noise-voltage density test is recommended when measuring noise on a large number of units. A 10Hz noise-voltage density measurement will correlate well with a 0.1Hz to 10Hz peak-to-peak noise reading since both results are determined by the white noise and the location of the 1/f corner frequency.

Current noise is measured in the circuit shown and calculated by the following formula where the noise of the source resistors is subtracted.

$$i_n = \frac{[e^2_{no} - (820nV)^2]^{1/2}}{40M\Omega \times 100}$$

0.1Hz to 10Hz Noise Test Circuit





APPLICATIONS INFORMATION

Frequency Compensation

The LT1008 is externally frequency compensated with a single capacitor. The two standard compensation circuits shown on page 3 are identical to the LM108A/308A frequency compensation schemes. Therefore, the LT1008 operational amplifiers can be inserted directly into LM108A/308A sockets, with similar AC and upgraded DC performance.

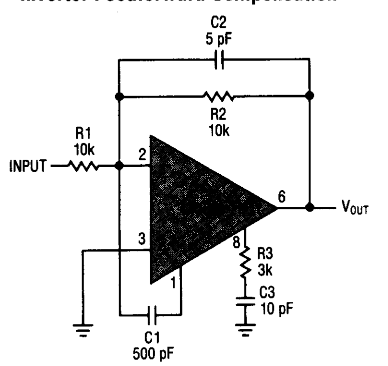
External frequency compensation provides the user with additional flexibility in shaping the frequency response of the amplifier. For example, for a voltage gain of ten, and $C_f = 3pF$, a gain bandwidth product of 5MHz and slew rate of 1.2V/μsec can be realized. For closed loop gains in excess of 200, no external compensation is necessary, and slew rate increases to 4V/μsec. The LT1008 can also be overcompensated (i.e. $C_f > 30pF$ or $C_S > 100pF$) to improve capacitive load handling capability or to narrow noise bandwidth. In many applications, the feedback loop around the amplifier has gain (e.g. logarithmic amplifiers); overcompensation can stabilize these circuits with a single capacitor.

The availability of the compensation terminals permits the use of feedforward frequency compensation to enhance slew rate in low closed loop gain configurations. The inverter slew rate is increased to 1.4V/μsec. The voltage follower feedforward scheme bypasses the amplifier's gain stages and slews at nearly 10V/μsec.

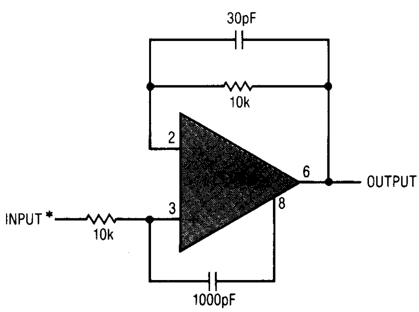
The inputs of the LT1008 are protected with back-to-back diodes. Current limiting resistors are not used, because the leakage of these resistors would prevent the realization of picoampere level bias currents at elevated temperatures. In the voltage follower configuration, when the input is driven by a fast, large signal pulse (> 1V), the input protection diodes effectively short the output to the input during slewing, and a current, limited only by the output short circuit protection will flow through the diodes.

The use of a feedback resistor, as shown in the voltage follower, feedforward diagram, is recommended because this resistor keeps the current below the short circuit limit, resulting in faster recovery and settling of the output.

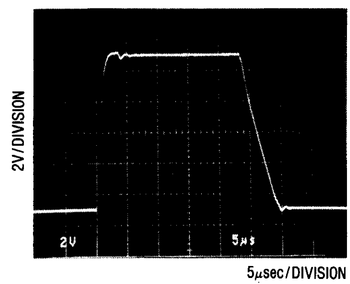
Inverter Feedforward Compensation

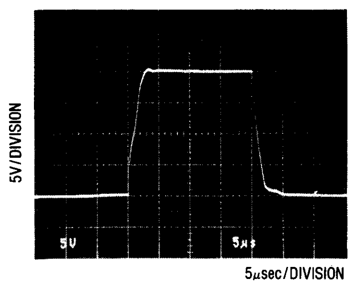


Follower Feedforward Compensation

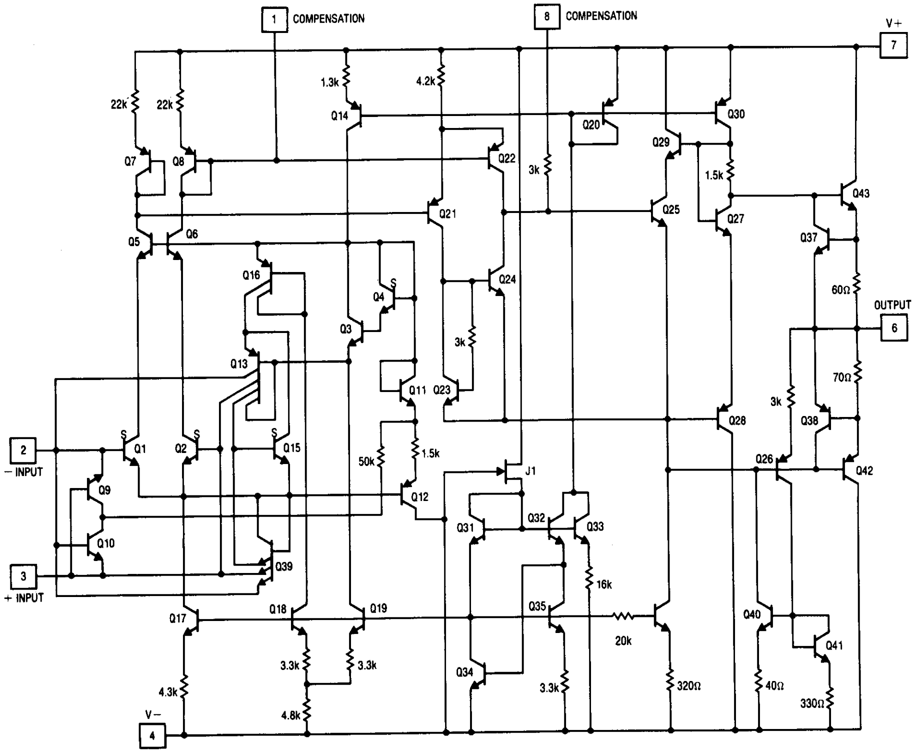


* SOURCE RESISTANCE ≤ 15k FOR STABILITY



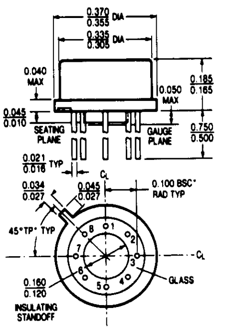


SCHEMATIC DIAGRAM



PACKAGE DESCRIPTION

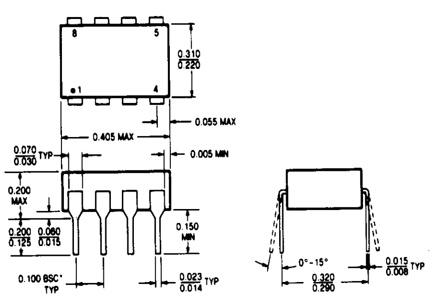
H Package Metal Can



NOTE: DIMENSIONS IN INCHES

$T_j$max	Θ_{ja}	Θ_{jc}
150°C	150°C/W	45°C/W

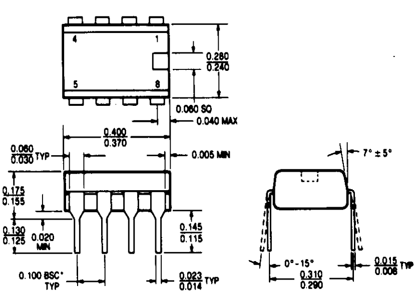
J8 Package 8 Lead Hermetic Dip



NOTE: DIMENSIONS IN INCHES UNLESS OTHERWISE NOTED.
*LEADS WITHIN 0.007 OF TRUE POSITION (TP) AT GAUGE PLANE

$T_j$max	Θ_{ja}
150°C	100°C/W

N8 Package 8 Lead Plastic



NOTE: DIMENSIONS IN INCHES UNLESS OTHERWISE NOTED.
*LEADS WITHIN 0.007 OF TRUE POSITION (TP) AT GAUGE PLANE.

$T_j$max	Θ_{ja}
100°C	130°C/W